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Systematic Design of Pseudo-Differential Frequency Filter

Ondrej Sladok

Department of Telecommunications
Brno University of Technology
Brno, Czech Republic
sladok@phd.feec.vutbr.cz

Jaroslav Koton

Department of Telecommunications
Brno University of Technology
Brno, Czech Republic
koton@feec.vutbr.cz

Martin Milota

Department of Telecommunications
Brno University of Technology
Brno, Czech Republic
xmilot03@stud.feec.vutbr.cz

Norbert Herencsar

Department of Telecommunications
Brno University of Technology
Brno, Czech Republic
herencsn@feec.vutbr.cz

Abstract — In the paper, the theory of systematic design frequency filters is described. The result is a fourth-order pseudo-differential frequency filter operating in the voltage-mode and implemented as a cascade connection of two basic second-order blocks. The filter is able to realize the low-pass filtering functions. The basic block employs three active elements and four passive elements. The filter is characterized by a minimum number of passive elements and high output impedance. Filter analysis examines the magnitude, phase, common-mode rejection ratio signal, and behavior of filters while reducing the recommended voltage. The proper functionality of the filter is verified by simulations and experimental measurements for two different interconnections.

Keywords — Pseudo-differential filter, voltage-mode, current conveyor, low-pass, cascade, systematic design

I. INTRODUCTION

Frequency filters are now an integral part of most electronic devices. Analog technology remains a little in the background compared to digital technology, which is recording great development. However, we must not forget this technique and therefore this article deals with one area of analog technology - frequency filters. Basic structures are used, the so-called single-ended circuits [1] – [2]. Interest in the design of fully-differential filters is growing, due to high demands for low-voltage and low-power applications [3] – [7]. Besides these applications, the emphasis is on improving the active elements or new development of these elements. For the design of new frequency filters, different types of active elements are used. As example, current feedback operational amplifiers (CFOAs) [8], current amplifiers (CAs) [9] – [10], operational transconductance amplifiers (OTAs) [11] – [13], current differential transconductance amplifiers (CDTAs) [14] or elements of the current conveyors (CCs) [15] - [23] can be mentioned. The advantages of fully-differential filters are, for example, enhances the dynamic range, the higher ability to reject power supply noise, reduced the harmonic distortion and reject the common-mode noise signals. On the other hand, the fully-differential filters exhibit generally double circuit complexity compared to single-ended solutions. Single-ended circuits have a simpler design but do not have the advantageous properties of fully-differential frequency filters, described above.

Therefore, pseudo-differential frequency filters [24] - [32] were proposed as a possible trade-off between fully-

differential and single-ended filters. They provide a simpler structure as single-ended circuits and provide similar features to fully-differential circuits.

In this paper, we deal with the systematic design of pseudo-differential filters working in the voltage-mode. The systematic approach is shown on the description and analysis of a fourth-order low-pass filter being designed as a cascade connection of two basic second-order blocks. The basic building block for systematic design is the second-order pseudo-differential frequency filter operating in the voltage-mode. The second-order filter uses three active elements - current conveyors and four passive elements. In theory, the input impedance of the filters is infinitely high and hence it is suitable for easy cascading. The cascade interconnection has been verified in two individual solutions, direct and cross interconnection of the two basic blocks. The analysis of the simulation and experimental results show the performance proving that the pseudo-differential frequency filter still features low sensitivity and the high common-mode rejection ratio. Simulation results also compared to experimental measurements prove the functionality of both cascade interconnection and support the theory of pseudo-differential filters.

II. PSEUDO-DIFFERENTIAL FILTERS

Pseudo-differential circuits combine the properties of fully-differential and single-ended filters. These structures have differential inputs and differential outputs, but the internal structure, in contrast with fully-differential circuits, remains non-differential. These structures do not contain as many elements as fully-differential circuits, therefore are less complex than fully-differential structures. Still, provide high suppression of the common-mode signal and have lower harmonic distortions. In practice, they are often used in combination with fully-differential filters [28].

As it is evident from the mathematical description (1) and the general view on voltage-mode fully-differential filters (Fig. 1a), only the differential input and differential output signals are assumed it. Therefore, it is generally possible to design differential system using differential input and differential outputs signals, where the inner structure is non-differential. These structures referred to as pseudo-differential filters (Fig. 1b)

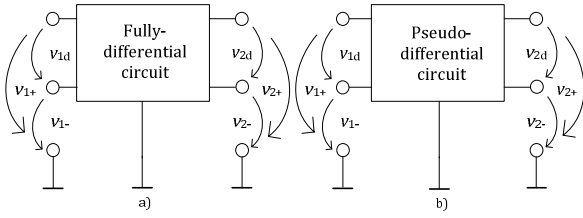


Fig. 1. a) Fully-differential structure, b) Pseudo-differential structure

are described by the following relations:

$$v_{1d} = v_{1+} - v_{1-}, \quad v_{2d} = v_{2+} - v_{2-}, \quad v_{1c} = \frac{v_{1+} + v_{1-}}{2}, \quad (1)$$

being also valid for fully-differential circuits whereas v_{1d} , v_{2d} and v_{1c} denote differential input voltage, the differential output voltage, and the common-mode input voltage, respectively. Signal v_{1d} is the difference between the two input signals v_{1+} and v_{1-} , while v_{1c} is expressing common-mode input signal as the average of the two input signals v_{1+} and v_{1-} . Taking into consideration (1), then the differential output voltage v_{2d} is defined as follows:

$$v_{2d} = v_{1d} \cdot A_{dm} + v_{1c} \cdot A_{cm}, \quad (2)$$

where A_{cm} and A_{dm} are common-mode and differential signal gains, respectively. The rejection of common-mode signal is expressed using $CMRR$ as [33]:

$$CMRR = 20 \log \left(\frac{A_{dm}}{A_{cm}} \right), \quad (3)$$

which determines the ability of an active element or a differential structure to suppress unwanted common-mode input signal that is common to both inputs, to the desired differential input signal. In ideal case $A_{cm} = 0$ and hence $CMRR$ is infinite.

III. SYSTEMATIC DESIGN OF PSEUDO-DIFFERENTIAL FILTERS

1) Description of CCII and DDCC

For the design of pseudo-differential frequency filter operating in voltage-mode the CCII and DDCC active elements have been used, which schematic symbols are shown in Fig. 2.

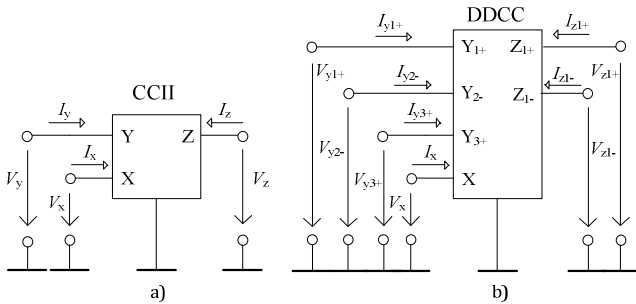


Fig. 2. a) Schematic symbols of CCII, b) Schematic symbols of DDCC

The CCII is a three-terminal building block with one

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high-impedance voltage input Y and low-impedance current input X, and one high-impedance current output Z.

The relation between terminal currents and voltages is given as [34]:

$$V_x = V_y, \quad I_y = 0, \quad I_z = I_x. \quad (4)$$

The DDCC is a six-terminal building block with three high-impedance voltage inputs Y_{1+} , Y_{2-} and Y_{3+} , a low-impedance current input X, and two high-impedance current outputs Z_{1+} and Z_{1-} . The relation between terminal currents and voltages is given as [34]:

$$V_x = V_{y1+} - V_{y2-} + V_{y3+}, \quad I_{y1+} = I_{y2-} = I_{y3+} = 0,$$

$$I_{z1+} = I_x, \quad I_{z1-} = -I_x. \quad (5)$$

2) Second-order pseudo-differential frequency filter

The basic block for systematic analysis is the second order pseudo-differential frequency filter. The circuit is realized using three active elements two DDCC and one CCII and four passive elements, where are all grounded. The differential input signal is directly led to the Y_{1+} and Y_{2-} terminals of DDCC1, Cascade connection is possible due to the high input impedance of the circuit and next advantage is the capacitors are not connected to terminals X, which in practice would result in additional parasitic poles.

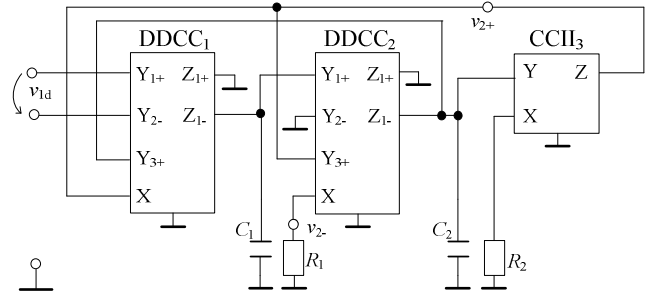


Fig. 3. Proposed second-order pseudo-differential frequency filter

Assuming the input and output nodes as denoted in Fig. 3, the structure allows realizing pseudo-differential second-order low-pass response since for the positive and negative output voltage v_{2+} and v_{2-} it holds:

$$v_{2+} = \frac{s^2 C_1 C_2 R_1 R_2 + 1}{s^2 C_1 C_2 R_1 R_2 + s C_1 R_2 + 1} \cdot v_{1d} + 0 \cdot v_{1c}, \quad (6a)$$

$$v_{2-} = \frac{s^2 C_1 C_2 R_1 R_2}{s^2 C_1 C_2 R_1 R_2 + s C_1 R_2 + 1} \cdot v_{1d} + 0 \cdot v_{1c}, \quad (6b)$$

and then for pseudo-differential-output voltage v_{2d} it can be written:

$$v_{2d} = \frac{1}{s^2 C_1 C_2 R_1 R_2 + s C_1 R_2 + 1} \cdot v_{1d} + 0 \cdot v_{1c}, \quad (6c)$$

if ideal active elements are considered. Comparing (6c) with

(2) we get differential gain:

$$A_{dm} = \frac{1}{s^2 C_1 C_2 R_1 R_2 + s C_1 R_2 + 1}, \quad (7)$$

3) Fourth-order pseudo-differential frequency filter

The proposed fourth-order pseudo-differential frequency filter was realized as the cascade connection of basic second-order blocks from Fig. 3.

The functionality of the filter was verified by two different connections of the basic blocks, i.e. direct and cross (Fig. 4).

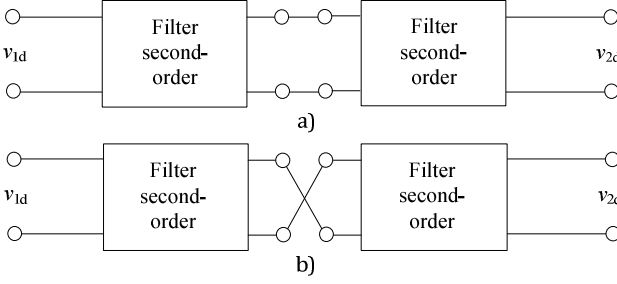


Fig. 4. Cascade connections a) Direct b) Cross

Direct and cross systematic designs in Fig. 4. have been subjected to simulations and experimental measurements. For both cascade connections, the low-pass response of the fourth-order pseudo-differential frequency filter can be described as:

$$A_{dm} = \frac{1}{s^4 (b_4) + s^3 (b_3) + s^2 (b_2) + s (b_1) + b_0}, \quad (8)$$

where

$$\begin{aligned} b_4 &= (C_{11}C_{12}C_{21}C_{22}R_{11}R_{12}R_{21}R_{22}), \\ b_3 &= (C_{12}C_{21}C_{22}R_{12}R_{21}R_{22} + C_{11}C_{12}C_{21}R_{11}R_{12}R_{21}), \\ b_2 &= (C_{11}C_{12}R_{11}R_{12} + C_{21}C_{22}R_{21}R_{22} + C_{12}C_{21}R_{12}R_{21}), \\ b_1 &= (C_{12}R_{12} + C_{21}R_{21}), b_0 = 1. \end{aligned}$$

IV. SIMULATIONS AND EXPERIMENTAL MEASUREMENTS

The behavior and performance of the proposed pseudo-differential filters have been evaluated by simulations. Furthermore, the behavior has been verified experimental measurements, was made for recommended supply voltages ($\pm 1.65V$) according to [38] and for reduced supply voltages ($\pm 1.50V$). The reduced supply voltage is a 90 percent value selected from the recommended supply voltage value. To realize the active elements CCII and DDCC, the universal current conveyor UCC-N1B 0520 [38] was used. Butterworth coefficients were used for the calculation of the 2nd- and 4th-order filters and pole-frequency $f_0 = 50kHz$.

1) Second-order pseudo-differential frequency filter

For simulations and experimental measurements the

values of capacitors $C_1 = C_2 = 1 \text{ nF}$ were selected and the values of resistors were determined as $R_1 = 2250\Omega$ and $R_2 = 4500\Omega$ to obtain the pole-frequency 50 kHz and quality factor $Q = 0.707$. The obtained frequency responses of the pseudo-differential second-order filter operating in voltage-mode are shown in Fig. 5.

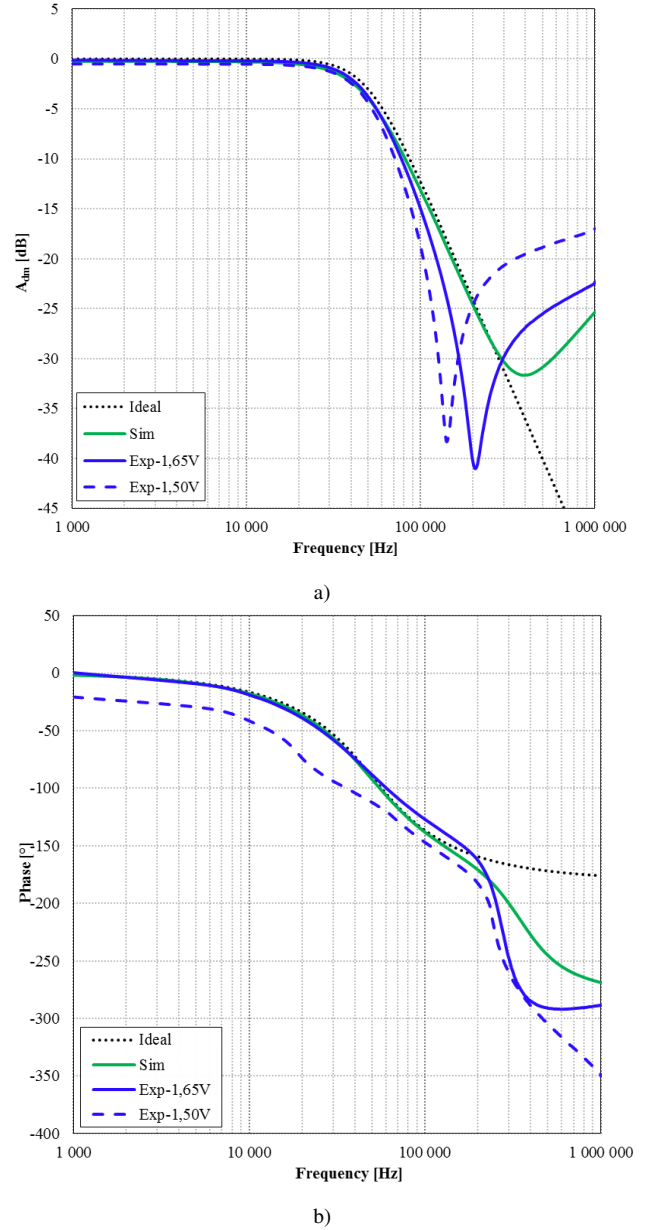


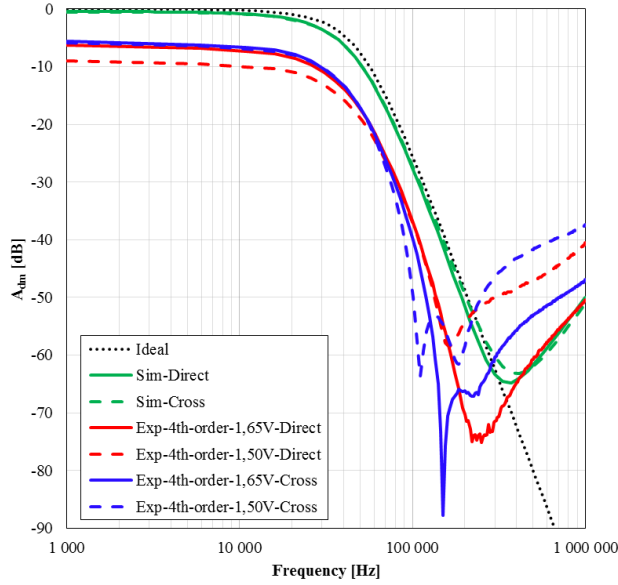
Fig. 5. Magnitude and phase characteristics of the low-pass second-order filter

From both the simulations and experimental measurements shown in Fig. 5 we can claim that they are in very good agreement with the theory. The worse result shows by measuring with reduced supply voltages but that is the expected behavior. Better result of the magnitude characteristic shows the experiment ($\pm 1.65V$), where the response is closer to the simulation. The real properties of the prototype cause a parasitic zero, which manifests around a frequency of approximately 200 kHz for simulations and experimental measurements.

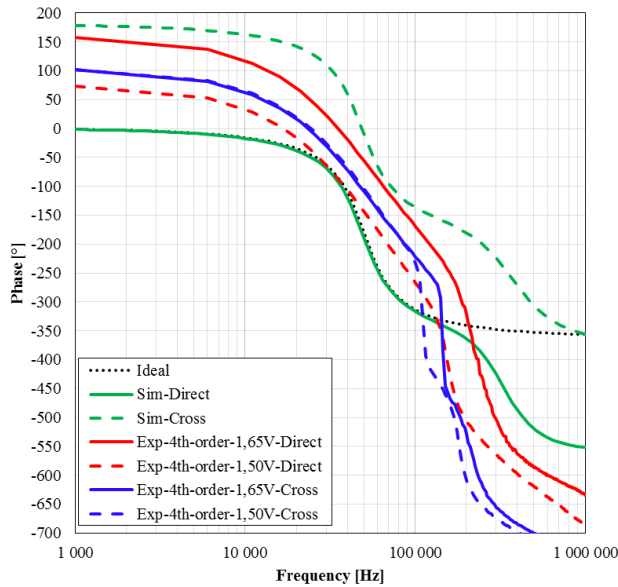
The phase characteristics for both supply voltage were achieving nearly ideal characteristics.

2) Fourth-order pseudo-differential frequency filter

The fourth-order pseudo-differential filter operating in the voltage mode was designed as a cascade connection of the basic second-order solution from Fig. 3. For simulations and measuring, Butterworth approximation was used. The values of capacitors $C_{11} = C_{12} = C_{21} = C_{22} = 1\text{nF}$ were selected and the resistor values $R_{11} = 1700\ \Omega$, $R_{12} = 5900\ \Omega$, $R_{21} = 2400\ \Omega$, $R_{22} = 4200\ \Omega$ were calculated resulting in 50 kHz pole-frequency. The plots in Fig. 6. show magnitude and phase characteristics.



a)



b)

Fig. 6. Magnitude and phase characteristics of the low-pass fourth-order filter

From the magnitude characteristics, it is clear that all experimental measurements are suppressed approximately 6 dB. The real properties of the integrated circuit at approximately 200 kHz were also reflected in the fourth-order filter. However, it is necessary to say that all responses copy to simulations characteristic.

From the phase characteristics in Fig. 6b) exhibit the greatest differences from all the results. Better result of the

phase characteristic shows the experiment ($\pm 1,65\text{V}$) - connection cross, but it has to be said that to the ideal transfer it is only approaching. The parasitic properties are caused by real properties of the active elements emulated by the UCC_N1B [38] simulation active elements.

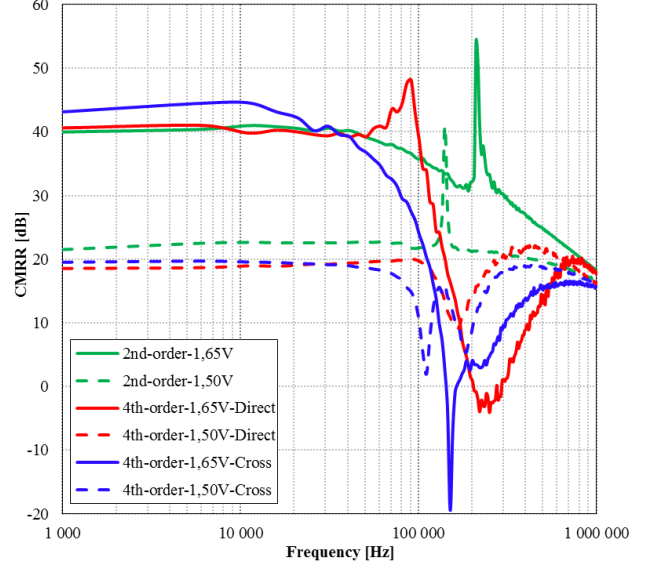


Fig. 7. The common-mode rejection ratio (CMRR) obtained by experimental measurements.

For both, pseudo-differential frequency filters (2nd-order and 4th-order) were measured the results and are shown in Fig. 7. The reached value of CMRR is approximately 40 dB and is constantly up to 200 kHz. The theoretical value of the common-mode rejection ratio is 43dB according to [28]. Drop around the frequency of 200 kHz is again a manifestation of real properties UCC-N1B 520 that create a parasitic zero. This phenomenon is already visible in the magnitude characteristics of Fig. 5a) and Fig. 6a), then the CMRR continues. When the supply voltage is reduced, the CMRR value is approximately 20dB. Therefore, the optimum supply voltage must be supplied for functionality.

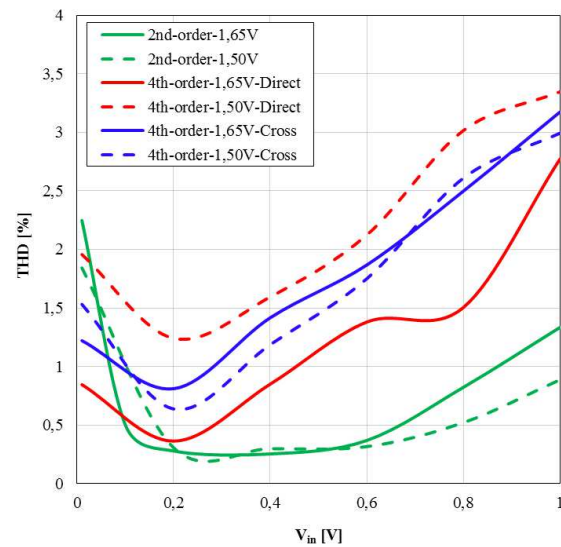


Fig. 8. Total harmonic distortion (THD) obtained by experimental measurements.

Next to CMRR the THD (total harmonic distortion) has

been measured. Evaluating THD, the first five major harmonic components were considered, whereas the 1 kHz input signal has been applied to V_{in} . As it can be seen in Fig. 8. for all experimental measurements, for input signal amplitude below 0.6 V the total harmonic distortion is less than 2%. For higher input signal amplitudes THD starts to decrease as the active elements start to reach their voltage and current saturation levels [38].

Simulations in PSpice evaluated the behavior and performance of the proposed pseudo-differential filters. They were then subjected to experimental measurements using an Agilent 4392A Network/Spectrum Analyzer. Other integrated circuits were used for experimental measurements. The AD8476 circuit [35] was used to obtain the input differential signal. Furthermore, two AD8271 summation amplifiers were used for the common-mode rejection ratio [36]. The output differential signal was converted to a single-ended signal using AD8429 [37]. The complete structure of the experimental measurement can be seen in Fig. 9., where is a block diagram of a pseudo-difference filter together with S/D and D/S converters and Fig. 10., where is the original design of the fourth-order pseudo-difference filter again together with the converters.

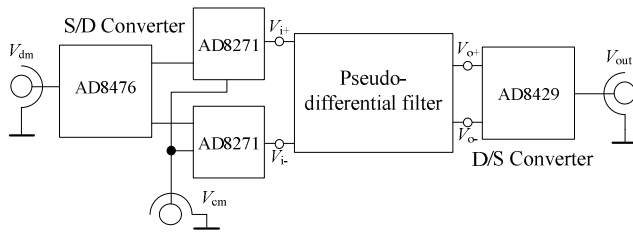


Fig. 9. The block diagram of the experimental measurement

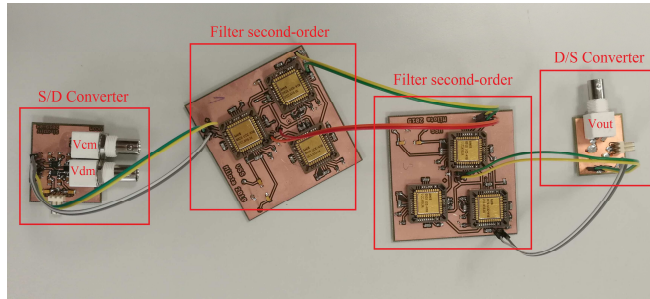


Fig. 10. The original design of the fourth-order pseudo-differential frequency filter

V. CONCLUSION

In this paper, a new systematic design of fourth-order pseudo-differential frequency filter operating in voltage mode is presented. The theory of pseudo-differential filters was investigated, where the possibility of designing higher-order filters was analyzed. Using the basic block - second-order pseudo-differential frequency filter connected in cascade, the fourth-order pseudo-differential filter operating in the voltage-mode was designed. The functionality and performance of the filter have been verified by both simulations and experimental measurements. Both the simulation and experimental measurements agree well with the theoretical analyses. The total harmonic distortion is less

than 2 % for the amplitude of the input signal below 0,6 V. The value of CMRR reached by measurements is approx. 40 dB. This article more confirms the theory of pseudo-differential frequency filters. This is proved by achieving generally the same results in the frequency response of the filter for direct and cross interconnections of the partial second-order blocks. Based on the presented results, it was shown that the theory of pseudo-differential filter is valid and fully functional.

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